

A METHOD AND APPARATUS FOR COMPENSATING FOR CABLE CHARGING EFFECTS ON CONTROL ALGORITHMS

CROSS-REFERENCE TO RELATED APPLICATIONS

[0001] Not applicable.

STATEMENT REGARDING FEDERALLY SPONSORED RESEARCH OR DEVELOPMENT

[0002] Not applicable.

BACKGROUND OF THE INVENTION

[0003] The field of the invention is motor controllers and more specifically methods and apparatuses for correcting phase and magnitude errors in motor control signals that result from cable/supply line charging effects. will indicate a signal associated with a stator q-axis in a d-q frame of reference

[0004] Throughout this specification a “*” will indicate a command signal, “ds” and “qs” subscripts will indicate signals associated with a stator q-axis in a d-q frame of reference, “u”, “v” and “w” subscripts will indicate values associated with three separate motor phases also referred to as u, v and w phases, a “f” subscript will indicate a feedback signal, a “s” subscript will indicate a motor stator quantity, a “NP” subscript will indicate a name plate value, an “a” subscript will indicate an angle, a “mag” subscript will indicate a magnitude value, an “o” subscript will indicate an output value and a “pd” subscript will indicate a predetermined or target value.

[0005] Referring to Fig. 1, a diagram 10 of a motor 14 and associated field oriented control (FOC) system is illustrated where the system includes a controller 11 and a pulse width modulating (PWM) inverter 12 linked to motor 14 via three voltage supply lines/cables 16, 18 and 20. In addition, simplified system 10 includes two input lines for supplying a command d-axis current I_{ds}^* and a torque command value or signal T_e^* and two current sensors 22 and 24 that sense currents on lines 18 and 20 and provide feedback currents I_{vf} and I_{wf} to controller 11.

[0006] Generally, controller 11 is programmed to receive the command values T_e^* and I_{ds}^* and use those values to generate voltages on supply lines 16, 18 and 20 that cause motor 14 to rotate in a manner that is consistent with the input command values. Feedback signals I_{vf} and I_{wf} form a closed loop that helps to drive motor 14 in the intended fashion. To this end, feedback signals I_{vf} and I_{wf} are converted into signals that can be compared to either the command signals or to derivatives of the command signals. Any differences between the commanded operating parameters and the feedback parameters are used to alter voltages applied across the supply lines appropriately. Thus, motor 14 rotates when a suitable torque command T_e^* and d-axis current command I_{ds}^* are provided. Similarly, torque command T_e^* may be set to zero and mechanical losses will then halt motor rotation.

[0007] As well known in the controls art, voltage equations in a d-q frame of reference can be expressed as follows:

$$V_{qs} = r_s I_{qs} + \omega_e L_s I_{ds} + d\lambda_{qs}/dt \quad \text{Eq. 1}$$

$$V_{ds} = r_s I_{ds} - \omega_e L_s I_{qs} + d\lambda_{ds}/dt \quad \text{Eq. 2}$$

where r_s is a stator resistance value, ω_e is a command frequency, L_s is a stator inductance, L_σ is a leakage inductance, λ_{qs} and λ_{ds} are flux values and I_{qs} and I_{ds} are q and d-axis currents, respectively.

[0008] Referring still to Fig. 1, the detail shown in controller 11 represents a common control algorithm for implementing Equations 1 and 2 above. To this end, controller 11 includes six summers 28, 34, 60, 58, 66 and 38, scalar gain values represented by blocks 30, 32, 44, 50, 54, 48 and 64, two multipliers 46 and 52, a torque to q-axis current converter 56, a proportional-integral (PI) regulator 62, an integrator 42, a polar converter 36, a polar to three phase converter 40 and a 3 to 2 phase converter 70.

[0009] Converter 70 receives feedback current signals I_{vf} and I_{wf} from line current sensors 24 and 26, uses the two received signals to determine the current in the third line 16 and converts the three phase currents to two phase d and q-axis feedback currents I_{dsf} and I_{qsf} , respectively. D-axis current I_{dsf} is provided to summer 28 and q-axis current I_{qsf} is provided to summer 60 and also to derivative with respect to time block 63.

[0010] D-axis command current I_{ds}^* is provided to summer 28 and the feedback current I_{dsf} is subtracted therefrom to generate a d-axis current error signal I_{dse} that is provided to and scaled by gain block 30. The scaled value generated by gain block 30 represents the change in d-axis flux with respect to time (i.e., the third term $d\lambda_{ds}/dt$ in Equation 2 above). The output of gain block 30 is provided to each of summer 34 and gain block 48.

[0011] Gain block 48 scales the received value thereby generating a value that represents the change in q-axis flux with respect to time (i.e., the third term $d\lambda_{qs}/dt$ in Equation 1 above) which is provided to summer 58. Command current I_{ds}^* is also provided to stator resistance gain block 32 and to stator inductance gain block 50, the outputs of which are provided to summer 34 and multiplier block 52, respectively.

[0012] Command torque value T_e^* is provided to converter 56 and, as the label implies, converter 56 converts command torque value T_e^* to a q-axis command current value I_{qs}^* . Command current value I_{qs}^* is provided to each of leakage inductance gain block 44, stator resistance gain block 54 and summer 60. The outputs of blocks 44 and 54 are provided to multiplier 46 and summer 58, respectfully.

[0013] Summer 60 subtracts q-axis current feedback value I_{qsf} from command current value I_{qs}^* to generate a q-axis current error value that is provided to regulator 62. Regulator 62 scales the received error signal to generate a command frequency value ω_e which is provided to each of multipliers 46 and 52 and summer 66.

[0014] Multiplier 46 multiplies the received values from block 44 and regulator 62 and provides its output to summer 34. Consistent with Equation 2 above, summer 34 subtracts value $\omega_e L_q I_{qs}$ (i.e., the output of multiplier 46) from the sum of the output values from gain blocks 32 and 30 to generate a d-axis voltage value V_{ds} . Voltage value V_{ds} is provided to polar converter 36. Similarly, multiplier 52 multiplies the values received from block 50 and regulator 62 and provides its output to summer 58. Summer 58 adds the received values to generate q-axis voltage value V_{qs} which is provided to polar converter 36.

[0015] Converter 36 converts the d and q-axis voltage values to a voltage magnitude signal V_{mag} and a voltage angle signal V_a . Magnitude signal V_{mag} is

provided to polar to three phase converter 40 and angle signal V_a is provided to summer 38.

[0016] Referring still to Fig. 1, block 63 takes the derivative of feedback current I_{qsf} thereby generating a compensation frequency in radians per second which is scaled by gain k_d at block 64. Summer 66 subtracts the scaled derivative of the q-axis feedback current value generated by block 64 from the output of regulator 62 and provides its output value to integrator 42. Integrator 42 integrates the received value to provide an electrical angle θ_e to summer 38. Summer 38 adds the voltage angle V_a and the electrical angle θ_e and provides its output to converter 40. Converter 40 converts the received magnitude value V_{mag} and adjusted angle value to three phase command values that are used to drive PWM inverter 12.

[0017] Methods for determining inductance values L_s and L_o are known in the art and will not be explained here in detail. Resistance value r_s is typically determined during a commissioning procedure by driving motor 14 with a name plate current I_{NP} at zero electrical frequency using both the d and q-axis current regulators, measuring an auto-tune voltage value V_{at1} (e.g., the output of a closed loop current regulator) and then solving the following equation:

$$r_s = V_{at1}/I_{NP} \quad \text{Eq. 3}$$

After determining resistance value r_s , that value is stored for subsequent use during motor control.

[0018] According to some control algorithms d-axis command current value I_{ds}^* is determined during a commissioning procedure by disconnecting the motor load from motor 14 and operating controller 11 at some reasonable operating frequency such as 75% of the rated motor name plate frequency. The resulting motor current is the no-load value of I_{ds}^* .

[0019] As well known in the motor control art, PWM inverters like inverter 12 include a plurality of switching devices that are controlled by controller 11 to generate voltage waveforms on supply cables 16, 18 and 20. With the advent of high speed switching devices and associated advantages, most power electronic inverters are now controlled so as to switch at very high speeds. Unfortunately, when high frequency switching is used to drive a motor 14 through relatively long

cables (e.g., several hundred feet), parasitic capacitance within the cables 16, 18 and 20 becomes significant. In fact, depending on the magnitude of the characteristic impedance of a cable configuration and system grounding, inverter 12 may have to provide a significant amount of energy to cables 16, 18 and 20 just to charge and discharge the cable capacitance. For a detailed explanation of cable charging and discharging phenomenon at high PWM switching frequencies see R. Kerkman, D. Leggate, G Skibinski, "Interaction of Drive Modulation and Cable Parameters on AC Motor Transients", IEEE Transactions on Industry Applications, Vol. 33, No. 3, May/June 1997, pp. 722 – 731.

[0020] Experience has shown that cable charging and discharging will, under certain circumstances, alter the switching characteristics of the power switching devices in PWM inverter 12. To this end, referring again to Fig. 1, it has been observed that, where cables 16, 18 and 20 are long (e.g., 500 feet) so that associated capacitance is appreciable, the feedback currents I_{vf} and I_{wf} at motor 14 (e.g., where the current sensors are located) are different than the currents provided by inverter 12 to the cables.

[0021] After cables 16, 18 and 20 become charged, the charged cables often generate unintended currents at the motor ends of the cables that are sensed by feedback sensors 24 and 26 and which end up hampering control efforts. At normal operating frequencies, while this phenomenon occurs, the distorting effect is relatively minimal due to the magnitude differences between the capacitive charge currents and the intended/generated currents. At low speeds, however, the distorting effects have larger relative magnitude, are more noticeable and have adverse effects on control. Specifically, when the torque command T_e^* is set to zero to stop motor 14, it has been observed that the feedback currents cause controller 11 to continue to generate non-zero torque and hence it is difficult to drive the motor to a stopped condition.

[0022] In this regard see Fig. 2 where two system characteristics are illustrated that were generated using a control algorithm similar to that illustrated in Fig. 1 with a 5 HP, 460 Volt AC, 4 pole motor and 11.0 Arms inverter with 600 feet of shielded motor cables 16, 18 and 20. The characteristics in Fig. 2 include a torque command value T_e^* and a resulting per unit operating or motor frequency f_o . It can be seen that at time τ_1 a step torque command is provided and frequency f_o begins

to rise as expected. At time τ_2 , torque command signal T_e^* is set equal to zero and frequency f_o begins to drop toward a zero value. However, at approximately time τ_3 , despite the zero torque value, output frequency f_o levels off at approximately .07 p.u.

[0023] Inability to reach a zero frequency after cable charging occurs is exacerbated by a d-axis command voltage error that is associated with the cable charging phenomenon described above. To this end, when torque command signal T_e^* is zero, Equations 1 and 2 above can be simplified as:

$$V_{qs} = \omega_e L_s I_{ds} + d\lambda_{qs}/dt \quad \text{Eq. 4}$$

$$V_{ds} = r_s I_{ds} \quad \text{Eq. 5}$$

Examining equations 4 and 5 it should be appreciated that with a zero torque command value, the applied voltage is dominated by the stator resistance drop and the correct value of I_{ds} . Thus, under test conditions with long cables and zero torque command, the open loop applied voltage in both the d-axis and the q-axis depend on the d-axis voltage resulting in the correct value of I_{ds} .

[0024] Referring still to Equation 5, as indicated above, resistance value r_s is determined during a commissioning procedure using the rated motor name plate current. Importantly, the commissioning test for stator resistance value r_s described above uses both the d and q-axis current regulators to identify resistance value r_s . The control method for normal system operation does not use both regulators and therefore actual values of d and q-axis currents cannot be forced to be identical to the commanded values. As discussed above, the cable charging effects distort the applied voltages on the motor terminals resulting in d-axis feedback current I_{dsf} that is generally greater than d-axis command current value I_{ds}^* at low operating frequencies without both the d and q-axis current regulators. Thus, the system described above generates an incorrect voltage value V_{ds} .

[0025] In addition to the effects of charging on long cables it is also believed that other drive operating characteristics can have exacerbating effects on the V_{ds} error. For instance, there is at least some evidence that non-ideal power device characteristics may add to the V_{ds} error described above.

BRIEF SUMMARY OF THE INVENTION

[0026] It has been recognized that, while the effects of charging on long cables occur at all operating frequencies, the relative magnitude of the effects on operating frequency are much greater and are relatively easily discernable at low operating frequencies and, indeed are determinable under zero torque command conditions. Thus, compensation angle for the voltage phase angle can be identified during a commissioning procedure by providing a zero torque command and, after the operating frequency reaches a steady state (e.g., deceleration stops), adjusting a compensation angle until the frequency is zero and then storing the adjusted compensation angle.

[0027] The invention includes a method for use with a three phase AC motor controller linked to a three phase motor, the controller receiving a torque command signal and generating a voltage phase angle as a function of the torque command signal, the voltage phase angle in turn used to generate modulating waveforms to drive a PWM inverter that provides voltages on three motor supply lines, the method comprising the steps of during a commissioning procedure, identifying at least one compensation angle that, when mathematically combined with the voltage phase angle, drives the motor to zero operating frequency when a zero torque command is received and, during normal operation and when a zero torque command is received, mathematically combining the compensation angle and the voltage phase angle to generate a compensated phase angle and using the compensated phase angle to generate the modulating waveforms.

[0028] In at least some embodiments the step of identifying a compensation angle includes driving the motor at a normal operating frequency, setting the torque command signal to zero, monitoring the motor frequency, when the motor stops decelerating, modifying the voltage phase angle until the motor frequency reaches zero and identifying the value by which the motor angle was modified to achieve zero speed as the compensation angle. Moreover, in some cases the step of modifying the voltage phase angle includes, when deceleration stops a) determining the operating frequency, b) negating the operating frequency to generate a frequency error value, c) integrating the frequency error value to generate an instantaneous compensation angle, d) mathematically combining the instantaneous compensation

angle and the voltage phase angle to generate a compensated phase angle, e) using the compensated phase angle to drive the motor; and f) repeating steps (a) through (e) until the operating frequency is zero.

[0029] In some embodiments the controller also generates d and q-axis voltage values as a function of the torque command signal and uses the d and q-axis voltage values to generate the voltage phase angle. Here, in some cases, the method is also for altering the d-axis voltage value to compensate for the effects of supply line capacitive charge on the d-axis voltage, the method further including the steps of mathematically combining the d-axis voltage value with a compensation factor to generate a compensated d-axis voltage value and using the compensated d-axis voltage value along with the q-axis voltage value to generate the voltage phase angle. Here, prior to normal operation and during a commissioning procedure, the method may include identifying the compensation factor and storing the compensation factor for use during normal operation. In one case the step of identifying the compensation factor includes driving the controller with a name plate current and measuring a first d-axis auto-tune voltage, identifying a no load d-axis current, driving the controller with the no load d-axis current and measuring a second d-axis auto-tune voltage and mathematically combining the first and second auto-tune voltages to generate the compensation factor. Here the step of mathematically combining the first and second auto-tune voltages may include dividing the second d-axis auto-tune voltage by the first d-axis auto-tune voltage and the step of mathematically combining the d-axis voltage value with a compensation factor to generate a compensated d-axis voltage value may include multiplying the compensation factor and the d-axis voltage value to generate the compensated d-axis voltage value.

[0030] The invention also includes an apparatus for use with a three phase AC motor controller linked to a three phase motor, the controller receiving a torque command signal and generating a voltage phase angle as a function of the torque command signal, the voltage phase angle in turn used to generate modulating waveforms to drive a PWM inverter that provides voltages on three motor supply lines, the apparatus comprising a processor running a program to perform the steps of, during a commissioning procedure, identifying at least one compensation angle that, when mathematically combined with the voltage phase angle, drives the motor

to zero operating frequency when a zero torque command is received and, during normal operation and when a zero torque command is received, mathematically combining the compensation angle and the voltage phase angle to generate a compensated phase angle and using the compensated phase angle to generate the modulating waveforms.

[0031] In some cases the processor performs the step of identifying a compensation angle by driving the motor at a normal operating frequency, setting the torque command signal to zero, monitoring the motor frequency, when the motor stops decelerating, modifying the voltage phase angle until the motor frequency reaches zero and identifying the value by which the motor angle was modified to achieve the zero speed as the compensation angle. Here, the processor may perform the step of modifying the voltage phase angle by, when deceleration stops: a) determining the operating frequency, b) negating the operating frequency to generate a frequency error value, c) integrating the frequency error value to generate an instantaneous compensation angle, d) mathematically combining the instantaneous compensation angle and the voltage phase angle to generate a compensated phase angle, e) using the compensated phase angle to drive the motor and f) repeating steps (a) through (e) until the operating frequency is zero.

[0032] In addition, the invention includes a method for use with a three phase AC motor controller linked to a three phase motor, the controller receiving a torque command signal and generating a voltage phase angle as a function of the torque command signal, the voltage phase angle in turn used to generate modulating waveforms to drive a PWM inverter that provides voltages on three motor supply lines, the method comprising the steps of during a commissioning procedure: a) driving the motor at a normal operating frequency, b) setting the torque command signal to zero, c) monitoring the motor frequency and, when the motor stops decelerating i) determining the operating frequency, ii) negating the operating frequency to generate a frequency error value, iii) integrating the frequency error value to generate an instantaneous compensation angle, iv) mathematically combining the instantaneous compensation angle and the voltage phase angle to generate a compensated phase angle, v) using the compensated phase angle to drive the motor and vi) repeating steps (i) through (v) until the operating frequency is zero, d) identifying the value by which the motor angle was modified to achieve the

zero speed as a compensation angle and during normal operation and when a zero torque command is received; e) mathematically combining the compensation angle and the voltage phase angle to generate a compensated phase angle and f) using the compensated phase angle to generate the modulating waveforms.

[0033] Here, the step of modifying the phase angle may include modifying the phase angle whenever any torque command is received.

[0034] These and other objects, advantages and aspects of the invention will become apparent from the following description. In the description, reference is made to the accompanying drawings which form a part hereof, and in which there is shown a preferred embodiment of the invention. Such embodiment does not necessarily represent the full scope of the invention and reference is made therefore, to the claims herein for interpreting the scope of the invention.

BRIEF DESCRIPTION OF THE SEVERAL VIEWS OF THE DRAWINGS

[0035] Fig. 1 is a diagram of a portion of a control system including the present invention linked to a motor;

[0036] Fig. 2 is a graph illustrating a torque command signal that may be provided to the controller of Fig. 1 and a resulting output frequency signal where the inventive compensation system is not employed;

[0037] Fig. 3 is a schematic diagram illustrating a voltage angle compensator according to the present invention;

[0038] Figs. 4(a) and 4(b) illustrate a flow chart according to one method of the present invention, wherein Fig. 4(a) illustrates a sub-method for identifying a d-axis voltage scalar value that compensates for control irregularities related to commissioned values of stator resistance and d-axis command current and Fig. 4(b) illustrates a sub-method for identifying a compensation angle for compensating for long cable charging effects;

[0039] Fig. 5 is a subassembly showing some detail of functional blocks in Fig. 1 consistent with the present invention;

[0040] Fig. 6 is a flow chart for use with a controller including the components of Figs. 1 and 5;

[0041] Fig. 7 is similar to Fig. 2, albeit illustrating waveforms generated where the inventive voltage magnitude compensation method has been activated;

[0042] Fig. 8 is similar to Fig. 2 albeit including a third waveform corresponding to a compensation angle generated via the angle compensation identification method of the present invention and wherein the angle compensation identification method is activated;

[0043] Fig. 9 is similar to Fig. 8, albeit illustrating the operating frequencies, correction angle and command torque waveforms during operation of one embodiment of the inventive method; and

[0044] Fig. 10 is similar to Fig. 5, albeit illustrating a second embodiment of various components.

DETAILED DESCRIPTION OF THE INVENTION

[0045] At least some embodiments of the present invention include two separate sub-processes including a first sub-process to identify a d-axis voltage correction factor ζ and a second sub-process to identify a voltage compensation angle δ . The sub-processes will first be described separately and then in conjunction. The first sub-process does not require additional or special hardware to identify factor ζ and therefore can be described without reference to any figures.

[0046] To compensate the d-axis voltage command V_{ds} for errors at low frequencies due to the commissioned value of resistance r_s and command current I_{ds} and the effects of cable charging with long lines, a correction factor ζ is identified by performing three steps. First, during the commissioning procedure to identify resistance value r_s , the measured auto-tune voltage when motor NP current is used to drive the load is stored as autotune voltage value V_{at1} . Second, after the no-load d-axis command current value I_{ds}^* is identified, value I_{ds}^* is used to drive the system and a second auto-tune voltage value V_{at2} is measured (e.g., the output of a closed loop current regulator is measured). Next, the second auto-tune voltage value V_{at2} is divided by the first auto-tune voltage value V_{at1} to generate correction factor ζ . Correction factor ζ is stored in a memory (see 121 in Fig. 5) for subsequent use.

[0047] Referring now to the drawings wherein like reference numerals correspond to similar elements throughout the several views and, more specifically, referring to Fig. 3, an exemplary assembly 80 for identifying compensation angle δ is illustrated. Assembly 80 is added to controller 11 in Fig. 1 during a commissioning

procedure and receives three signals including voltage angle value V_a , q-axis feedback current I_{qsf} and torque command value T_e^* . Assembly 80 includes summers 82 and 85, a single pole, double throw switch 83, a proportional-integral (PI) regulator 88 and a system observer 160. System observer 160 in turn includes a frequency determiner 84 and a deceleration identifier 86.

[0048] Observer 160 receives two input values including the q-axis feedback current value I_{qsf} and the command torque value T_e^* and operates during a commissioning procedure to perform two functions. First, observer 160 determines system output frequency f_o (e.g., motor frequency). Second, observer 160 determines when the output frequency stops decelerating after a zero command torque value T_e^* is provided. To determine frequency f_o , observer 160 includes a frequency determiner 84 that uses q-axis feedback current value I_{qsf} to determine the instantaneous motor operating frequency f_o as well known in the art. Other ways to determine frequency f_o (e.g., a commissioning encoder, etc.) are contemplated and the present invention should not be limited by how frequency f_o is determined.

[0049] The output value f_o is provided to each of summer 82 and identifier 86. Identifier 86 compares an instantaneous or filtered output frequency $f_o t(n)$ to a previous output frequency value $f_o t(n-1)$ when the command torque value T_e^* is zero and, when the two values match, generates a switch control signal that is provided to switch 83.

[0050] Summer 82 subtracts output frequency value f_o from a zero value and generates an error output frequency value f_e . The output of summer 82 is provided to switch 83. Switch 83 is normally open and, when a control signal is received from identifier 86, switch 83 closes thereby providing the error output frequency f_e to PI regulator 88. Regulator 88 scales the received value thereby generating compensation angle δ . Compensation angle δ is provided to summer 85 which also receives polar angle V_a (see again Fig. 1). Summer 85 adds compensation angle δ to angle V_a and generates a corrected angle value V'_a which is provided in Fig. 1 to summer 38. Thus, generally, during the second commissioning sub-process, when a zero torque command T_e^* is provided to controller 11, once motor 14 stops decelerating, switch 83 is closed and frequency value f_e is scaled to generate compensation angle δ . Compensation angle δ is increased or decreased until output

frequency f_0 is zero (i.e., motor 14 stops). Value δ is stored in memory 121 (see Fig. 5) for subsequent use.

[0051] Referring now to Figs. 4(a) and 4(b), a more detailed method 90 consistent with the comments above is illustrated. In Fig. 4(a), beginning at block 91, first auto-tune voltage value V_{at1} is stored during the commissioning procedure to identify resistance value r_s . Next, at block 92, flux current command I_{ds}^* is used to drive controller 11 and, at block 94, the voltage on the output of the current regulator is measured to identify second auto-tune voltage V_{at2} . At block 95, a d-axis voltage correction factor ζ is identified by dividing auto-tune voltage V_{at2} corresponding to the flux current I_{ds}^* by auto-tune voltage V_{at1}^* corresponding to the nameplate current. Correction value ζ is stored at block 95.

[0052] After block 95, control passes to block 96. Correction factor ζ is used to modify the d-axis voltage value V_{ds} during the second commissioning sub-process. To this end, referring to Figs. 5 and 6 and again to Fig. 1, a V_{ds} compensator 69 is linked to memory 121 to receive value ζ and includes multiplier 154. Multiplier 154 receives value ζ and, at block 96, multiplies the d-axis voltage value V_{ds} from summer 34 in Fig. 1 by factor ζ to compensate for the d-axis voltage error as described above. The output V'_{ds} of multiplier 154 is provided to polar converter 156.

[0053] Referring to Fig. 4(b), with factor ζ stored and compensator 69 activated, at block 101, a non-zero torque command value T_e^* and flux current value I_{ds}^* are provided to controller 11 to drive motor 14. Controller 11 uses the command values and feedback current values to generate q and d-axis voltage command signals V_{qs} and V_{ds} , respectively. Q-axis value V_{qs} is provided directly to polar converter 36. D-axis value V_{ds} , as illustrated, is provided to V_{ds} compensator 69 to generate compensated value V'_{ds} .

[0054] At block 102, converter 36 identifies voltage angle V_a by taking the arc tangent of the ratio of the q-axis voltage command value V_{qs} divided by the d-axis voltage value V'_{ds} . In addition, at block 104, polar converter 36 identifies the magnitude V_{mag} of a polar voltage corresponding to the q-axis command voltage and value V'_{ds} by taking the square root of the sum of the squares of voltages V_{qs} and V'_{ds} . At block 106, the magnitude and angle values V_{mag} and V_a are used to drive motor 14 (e.g., compensator 71 is not yet activated).

[0055] At block 110, output frequency f_o is monitored and compared to a predetermined or target frequency f_{pd} which, for instance, may be 25% of the rated operating frequency. Where frequency f_o is not equal to or greater than the predetermined frequency f_{pd} , control passes back up to block 102 where the voltage angle and magnitude signals are recalculated and used to drive motor 14. The loop including blocks 102, 104, 106 and 110 is repeated until output frequency f_o is greater than or equal to the predetermined frequency f_{pd} at which point control passes to block 112.

[0056] At block 112, command torque T_e^* is set equal to zero. At block 116 in Fig. 3, frequency f_o is compared to zero. At block 118, deceleration identifier 86 determines whether or not motor 14 has stopped decelerating by comparing consecutive output frequency values $f_o(t(n-1))$ and $f_o(t(n))$. Where motor 14 is continuing to decelerate, control passes back up to block 116 and the loop including blocks 116 and 118 continues. At block 118, once system deceleration stops, control passes to block 122. Referring also to Fig. 3, at block 122, the frequency error f_e (i.e., the negated output frequency f_o) is provided to PI regulator 88 by closing switch 83.

[0057] After block 122, control passes to block 124 where frequency error f_e is scaled to generate compensation angle δ . At block 126, the voltage angle V_a is recomputed by adding compensation angle δ to the newly computed arc tangent of ratio V_{aqs}/V_{ds} . After block 126 control passes again to block 104 where voltage magnitude V_{mag} is determined and then loops back down through the lower part of the flow chart as illustrated.

[0058] Referring once again to block 116, eventually, as the magnitude of compensation angle δ is increased or decreased, output frequency f_o is driven toward and reaches zero. When output frequency f_o is zero, control passes from block 116 to block 120 where compensation angle δ is stored in memory 121 for use.

[0059] Referring again to Fig. 5, according to at least one embodiment of the invention, the components in Fig. 5 are added (e.g., typically through modification to software) to the components of Fig. 1 and values δ and ζ are set as described above. The components of Fig. 5 include previously described memory 121 and V_{ds} compensator 69 that receives the V_{ds} value from summer 34 (see again Fig. 1) and

value ζ and multiplies those values to generate modified V'_{ds} value that is provided to polar converter 156. In addition, Fig. 5 also includes voltage angle compensator 71 that is linked to memory 121 to receive compensation angle δ and includes a summer 162. Summer 162 receives the voltage angle V_a from converter 156 and adds angle δ to angle V_a to generate a modified or compensated voltage angle value V'_a . V'_a is provided to summer 38 during normal system operation.

[0060] Referring now to Fig. 6, a method for use with controller 11 of Fig. 1 including the compensators of Fig. 5 is illustrated. In Fig. 6, it is assumed that, initially, a d-axis command current value I_{ds}^* and a non-zero torque command value T_e^* are provided to controller 11 so that motor 14 is being driven at some operating frequency. At block 133, the d-axis voltage compensator 69 multiplies compensator factor ζ by the d-axis voltage value V_{ds} to generate the compensated d-axis voltage V'_d . At block 134 converter 36 identifies magnitude value V_{mag} as the square root of the sum of the squares of value V_{qs} and value V'_{ds} . In addition, at block 134 converter 36 identifies angle V_a as the arc tangent of ratio V_{qs}/V'_{ds} . At block 132, compensator 71 adds compensator angle δ to voltage angle V_a to generate compensated voltage angle V'_a . At block 136 magnitude V_{mag} and angle V'_a values are provided to converter 40 and summer 38, respectively, and hence are used to drive motor 14. The process of Fig. 6 is repeated.

[0061] Referring now to Fig. 7, exemplary waveforms similar to the waveforms described above with respect to Fig. 2 are illustrated, included an output frequency waveform f_o and a torque command waveform T_e^* . The waveforms in Fig. 7 were generated with a system similar to the system used to generate the waveforms in Fig. 2 except that the d-axis voltage correcting sub-method of the present invention (e.g., Fig. 4(a) and compensator 69) was activated (i.e., compensator angle δ portion of the present invention was disabled). As illustrated, the d-axis voltage correction sub-method reduced the output frequency error from 0.07 p.u. to approximately 0.06 p.u. Thus, d-axis voltage correction alone is useful but not sufficient to fully compensate for cable charging effects.

[0062] Referring to Fig. 8, waveforms generated during a commissioning procedure with a system like the system described above with respect to Fig. 2 are

illustrated where the angle compensation sub-method of the present invention was activated. In Fig. 8, like Fig. 2, an output frequency waveform f_o and a torque command waveform T_e^* are illustrated. In addition, a compensation angle waveform δ is illustrated. As in Fig. 2, at time τ_1 a non-zero torque command T_e^* is provided which causes output frequency f_o to increase. At time τ_2 the torque command T_e^* is set to zero and output frequency f_o begins to decrease. At approximately time τ_3 , prior to the output frequency reaching a zero value, output frequency f_o levels off. Once output frequency f_o levels off, the compensation angle δ generated by PI regulator 88 in Fig. 3 begins to decrease. Eventually, at approximately τ_4 , compensation angle δ reaches a level that causes output frequency f_o to be driven to a zero value. Thus, the correction value δ corresponding to τ_4 , is stored for subsequent use.

[0063] Fig. 9 is similar to Fig. 8, albeit illustrating waveforms generated during normal system operation (i.e., post commissioning) where both the angle and voltage magnitude compensators have been enabled. In Fig. 9, at time τ_1 , a non-zero torque command T_e^* is used to drive controller 11. When command value T_e^* is provided, frequency f_o rises. In addition, compensator angle δ is added to the voltage angle V_a to generate compensated voltage angle V_a' (i.e., the angle compensator is activated). At time τ_2 torque command value T_e^* is set to zero and frequency f_o begins to decrease. While frequency f_o is decreasing the angle compensator remains activated. Eventually and generally in a linear fashion with minimal leveling off of frequency f_o , operating frequency f_o reaches zero at time τ_3 .

[0064] In addition to the system and method described above, according to another aspect of the invention, a table of compensation angle δ values may be generated that is used during a load stopping procedure. To this end, referring again to Fig. 8, during the commissioning process to identify value δ , there are several intermediate times between τ_3 and τ_4 during which, as value δ is decreased, deceleration levels off at intermediate levels. For instance, between times τ_5 and τ_6 , with a first value δ_1 , deceleration levels off, between times τ_5 and τ_6 with a second value δ_2 , deceleration may again level off and so on. In Fig. 8, there are five separate δ values $\delta_1 - \delta_5$ between times τ_3 and τ_4 . Here, the frequencies at which deceleration levels off and corresponding δ values may be stored in a table form and

used to activate the δ compensation feature differently at different operating frequencies to increase the level of control during stopping.

[0065] In this regard see Fig. 10 that illustrates one additional embodiment including a memory 200 having, in addition to the ζ value, a δ -frequency table 202. In addition to including the enhanced memory 200, Fig. 10 also includes a determiner 204 that uses the q-axis current value I_{qsf} to identify instantaneous operating frequency and a δ selector 206. Selector 206 is linked to each of memory 200 and determiner 204. In this embodiment, during the commissioning procedure, once deceleration stops, the frequency of at which the deceleration stopped is stored as first frequency f_{o1} . For instance, the frequency f_{o1} may be 5Hz. Next, a first small δ value (e.g., δ_1) is correlated with the first frequency f_{o1} and stored therewith. The first value δ_1 is then provided as an intermediate compensation angle to be added to the voltage phase angle to generate a compensated voltage phase angle which is in turn used to drive the motor.

[0066] Again, the operating frequency is monitored and the frequency at which deceleration stops is determined and stored as a second frequency f_{o2} (e.g., 3Hz). Thereafter, the magnitude of first compensation value δ_1 is increased to generate the second value δ_2 which is again used to modify the voltage phase angle and to drive the motor. The second value δ_2 is correlated and stored with the second frequency f_{o2} . This process is repeated until the operating frequency is zero and complete δ - f_o table 202 has been constructed.

[0067] Referring still to Fig. 10, components labeled with identical numbers in Figs. 10 and 5 have similar operations and therefore are not again explained here in detail. During normal operation with the Fig. 10 components added to the Fig. 1 components, frequency determiner 204 uses q-axis feedback current I_{qsf} to identify an instantaneous operating frequency f_o . Selector 206 uses the instantaneous operating frequency f_o to identify a corresponding δ value in table 202 to be added to the polar angle V_a to generate compensated value V'_a . Thus, using the components of Fig. 10, the δ value is adjusted when frequency of deceleration stalls and the stopping process is relatively soft.

[0068] It should be understood that the methods and apparatuses described above are only exemplary and do not limit the scope of the invention, and that

various modifications could be made by those skilled in the art that would fall under the scope of the invention. For example, referring to Fig. 1 again, instead of adding angle δ between converter 36 and summer 38, the angle could be added after summer 38 or between integrator 42 and summer 38. Other modifications are contemplated.

[0069] To apprise the public of the scope of this invention, the following claims are made: